

Shunt Active Power Filter for Power Quality Improvement By SAPF Using PV System



B.Surendhar

**M.Tech Student,
Control Systems,**

**Lords College of Engineering and Technology,
Hyderabad, Telangana, India.**



K.Ramu

Assistant Professor,

**Dept of Electrical Engineering
Lords College of Engineering and Technology,
Hyderabad, Telangana, India.**

Abstract:

Traditionally, active power filters have been controlled using pretuned controllers, such as PI-type or adaptive, for the current as well as for the dc-voltage loops. Active power filters implemented with three-phase four-leg voltage-source inverters (4L-VSI) have already been presented in the technical literature, the primary contribution of this paper is a predictive control algorithm designed and implemented specifically for this application. PI controllers must be designed based on the equivalent linear model, while predictive controllers use the nonlinear model, which is closer to real operating conditions. A detailed yet simple mathematical model of the active power filter, including the effect of the equivalent power system impedance, is derived and used to design the predictive control algorithm.

Key words:

Shunt active filter, harmonics, active power, power quality, solar energy.

I.INTRODUCTION:

RENEWABLE generation affects power quality due to its nonlinearity, since solar generation plants and wind power generators must be connected to the grid through high-power static PWM converters. The non-uniform nature of power generation directly affects voltage regulation and creates voltage distortion in power systems. This new scenario in power distribution systems will require more sophisticated compensation techniques. Although active power filters implemented with three-phase four-leg voltage-source inverters (4L-VSI) have already been presented in the technical literature, the primary contribution of this paper is a predictive control algorithm designed and implemented specifically for this application.

Traditionally, active power filters have been controlled using pretuned controllers, such as PI-type or adaptive, for the current as well as for the dc-voltage loops. PI controllers must be designed based on the equivalent linear model, while predictive controllers use the nonlinear model, which is closer to real operating conditions. An accurate model obtained using predictive controllers improves the performance of the active power filter, especially during transient operating conditions, because it can quickly follow the current-reference signal while maintaining a constant dc-voltage. So far, implementations of predictive control in power converters have been used mainly in induction motor drives. In the case of motor drive applications, predictive control represents a very intuitive control scheme that handles multivariable characteristics, simplifies the treatment of dead-time compensations, and permits pulse-width modulator replacement. However, these kinds of applications present disadvantages related to oscillations and instability created from unknown load parameters.

One advantage of the proposed algorithm is that it fits well in active power filter applications, since the power converter output parameters are well known. These output parameters are obtained from the converter output ripple filter and the power system equivalent impedance. The converter output ripple filter is part of the active power filter design and the power system impedance is obtained from well-known standard procedures. In the case of unknown system impedance parameters, an estimation method can be used to derive an accurate R-L equivalent impedance model of the system. This paper presents the mathematical model of the 4L-VSI and the principles of operation of the proposed predictive control scheme, including the design procedure. The complete description of the selected current reference generator implemented in the active power filter is also presented.

Finally, the proposed active power filter and the effectiveness of the associated control scheme compensation are demonstrated through simulation results.

II.CONVERTER DESCRIPTION:

Both types of power generation use ac/ac and dc/ac static PWM converters for voltage conversion and battery banks for long term energy storage. These converters perform maximum power point tracking to extract the maximum energy possible from wind and sun. The electrical energy consumption behavior is random and unpredictable, and therefore, it may be single- or three-phase, balanced or unbalanced, and linear or nonlinear. An active power filter is connected in parallel at the point of common coupling to compensate current harmonics, current unbalance, and reactive power. It is composed by an electrolytic capacitor, a four-leg PWM converter, and a first-order output ripple filter, as shown in Fig. 1.

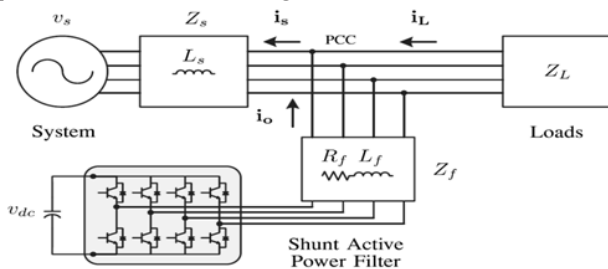


Figure 1: Three-phase equivalent circuit of the proposed shunt active power filter.

This circuit considers the power system equivalent impedance Z_s , the converter output ripple filter impedance Z_f , and the load impedance Z_L . The four-leg PWM converter topology is shown in Fig. 2. The voltage in any leg x of the converter, measured from the neutral point (n), can be expressed in terms of switching states, as follows:

$$V_{xn} = S_x - S_n V_{dc}, \quad x = u, v, w, n.$$

The mathematical model of the filter derived from the equivalent circuit shown in Fig. 3 is

$$V_o = V_{xn} - R_{eq} i_o - L_{eq} (di_o/dt)$$

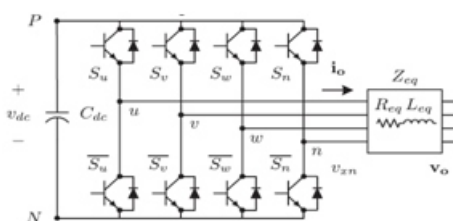


Figure 2: Two-level four-leg PWM-VSI topology

Where R_{eq} and L_{eq} are the 4L-VSI output parameters expressed as Thevenin impedances at the converter output terminals Z_{eq} . Therefore, the Thevenin equivalent impedance is determined by a series connection of the ripple filter impedance Z_f and a parallel arrangement between the system equivalent impedance Z_s and the load impedance Z_L .

$$Z_{eq} = \frac{Z_s Z_L}{Z_s + Z_L} + Z_f \approx Z_s + Z_f$$

For this model, it is assumed that $Z_L > Z_s$, that the resistive part of the system's equivalent impedance is neglected, and that the series reactance is in the range of 3–7% p.u., which is an acceptable approximation of the real system. Finally, $R_{eq} = R_f$ and $L_{eq} = L_s + L_f$.

III.CONTROL STRATEGY:

Digital predictive current control:

The block diagram of the proposed digital predictive current control scheme is shown in Fig. 3. This control scheme is basically an optimization algorithm and, therefore, it has to be implemented in a microprocessor. Consequently, the analysis has to be developed using discrete mathematics in order to consider additional restrictions such as time delays and approximations. The main characteristic of predictive control is the use of the system model to predict the future behavior of the variables to be controlled. The controller uses this information to select the optimum switching state that will be applied to the power converter, according to predefined optimization criteria. The predictive control algorithm is easy to implement and to understand, and it can be implemented with three main blocks, as shown in Fig. 3.

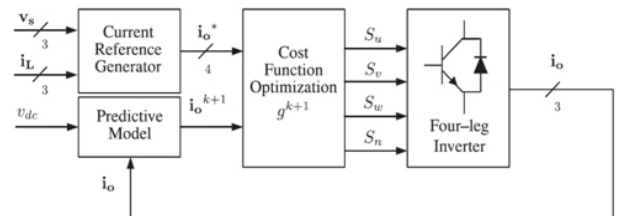


Figure 3: Proposed predictive digital current control block diagram

Current Reference Generator:

This unit is designed to generate the required current reference that is used to compensate the undesirable load current components.

In this case, the system voltages, the load currents, and the dc-voltage converter are measured, while the neutral output current and neutral load current are generated directly from these signals.

Prediction Model:

The converter model is used to predict the output converter current. Since the controller operates in discrete time, both the controller and the system model must be represented in a discrete time domain. The discrete time model consists of a recursive matrix equation that represents this prediction system. This means that for a given sampling time T_s , knowing the converter switching states and control variables at instant kT_s , it is possible to predict the next states at any instant $[k + 1]T_s$.

Due to the first-order nature of the state equations that describe the model, a sufficiently accurate first-order approximation of the derivative is considered in this paper. In order to predict the output current i_o at the instant $(k + 1)$, the input voltage value V_o and the converter output voltage V_{xN} , are required. The algorithm calculates all 16 values associated with the possible combinations that the state variables can achieve.

Cost Function Optimization:

In order to select the optimal switching state that must be applied to the power converter, the 16 predicted values obtained for $i_o[k + 1]$ are compared with the reference using a cost function g , as follows:

$$g[k + 1] = (i^*_{ou}[k + 1] - i_{ou}[k + 1])^2 + (i^*_{ov}[k + 1] - i_{ov}[k + 1])^2 + (i^*_{ow}[k + 1] - i_{ow}[k + 1])^2 + (i^*_{on}[k + 1] - i_{on}[k + 1])^2$$

The output current (i_o) is equal to the reference (i^*_o) when $g = 0$. Therefore, the optimization goal of the cost function is to achieve a g value close to zero. The voltage vector v_{xN} that minimizes the cost function is chosen and then applied at the next sampling state. During each sampling state, the switching state that generates the minimum value of g is selected from the 16 possible function values. The algorithm selects the switching state that produces this minimal value and applies it to the converter during the $k + 1$ state.

Current reference generation:

A dq-based current reference generator scheme is used to obtain the active power filter current reference signals. This scheme presents a fast and accurate signal tracking capability. This characteristic avoids voltage fluctuations that deteriorate the current reference signal affecting compensation performance. The current reference signals are obtained from the corresponding load currents as shown in Fig. 4. This module calculates the reference signal currents required by the converter to compensate reactive power, current harmonic and current imbalance. The displacement power factor ($\sin \phi(L)$) and the maximum total harmonic distortion of the load (THD(L)) defines the relationships between the apparent power required by the active power filter, with respect to the load, as shown

$$\frac{S_{APF}}{S_L} = \frac{\sqrt{\sin^2 \phi(L) + THD(L)^2}}{\sqrt{1 + THD(L)^2}}$$

Where the value of THD(L) includes the maximum compensable harmonic current, defined as double the sampling frequency f_s . The frequency of the maximum current harmonic component that can be compensated is equal to one half of the converter switching frequency.

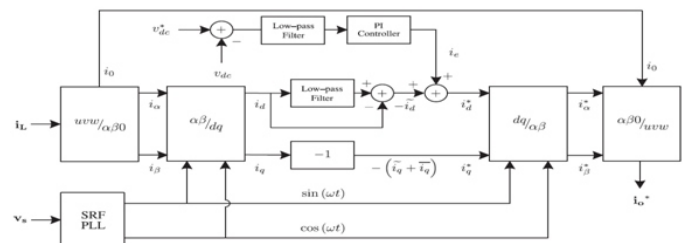


Figure 4: dq-based current reference generator block diagram.

Where the value of THD(L) includes the maximum compensable harmonic current, defined as double the sampling frequency f_s . The frequency of the maximum current harmonic component that can be compensated is equal to one half of the converter switching frequency. The dq-based scheme operates in a rotating reference frame; therefore, the measured currents must be multiplied by the $\sin(\omega t)$ and $\cos(\omega t)$ signals. By using dq-transformation, the d current component is synchronized with the corresponding phase-to-neutral system voltage, and the q current component is phase-shifted by 90° . The $\sin(\omega t)$ and $\cos(\omega t)$ synchronized reference signals are obtained from a synchronous reference frame (SRF) PLL.

The SRF-PLL generates a pure sinusoidal waveform even when the system voltage is severely distorted. Tracking errors are eliminated, since SRF-PLLs are designed to avoid phase voltage unbalancing, harmonics (i.e., less than 5% and 3% in fifth and seventh, respectively), and offset caused by the nonlinear load conditions and measurement errors. Allow-pass filter (LFP) extracts the dc component of the phase currents i_d to generate the harmonic reference components $-i_d$. The reactive reference components of the phase-currents are obtained by phase-shifting the corresponding ac and dc components of i_q by 180° . In order to keep the dc-voltage constant, the amplitude of the converter reference current must be modified by adding an active power reference signal i_e with the d-component, as will be explained in Section IV-A. The resulting signals i^*d and i^*q are transformed back to a three-phase system by applying the inverse Park and Clark transformation. The cutoff frequency of the LPF used in this paper is 20 Hz.

The current that flows through the neutral of the load is compensated by injecting the same instantaneous value obtained from the phase-currents, phase-shifted by 180° , as shown next $i^*on = -(iLu + iLv + iLw)$. One of the major advantages of the dq-based current reference generator scheme is that it allows the implementation of a linear controller in the dc-voltage control loop. The amplitude of this harmonic depends on the percent of unbalanced load current (expressed as the relationship between the negative sequence current $iL,2$ and the positive sequence current $iL,1$). The second-order harmonic cannot be removed from i_d and i_q , and therefore generates a third harmonic in the reference current when it is converted back to abc frame. Since the load current does not have a third harmonic, the one generated by the active power filter flows to the power system.

DC-Voltage Control:

The dc-voltage converter is controlled with a traditional PI controller. This is an important issue in the evaluation, since the cost function is designed using only current references, in order to avoid the use of weighting factors. Generally, these weighting factors are obtained experimentally, and they are not well defined when different operating conditions are required. The dc-voltage remains constant (with a minimum value of $\sqrt{6}Vs(\text{rms})$) until the active power absorbed by the converter decreases to a level where it is unable to compensate for its losses.

The active power absorbed by the converter is controlled by adjusting the amplitude of the active power reference signal i_e , which is in phase with each phase voltage. In the block diagram shown in Fig. 5, the dc-voltage v_{dc} is measured and then compared with a constant reference value v^*dc . Fig. 5 shows that the output of the PI controller is fed to the dc-voltage transfer function G_s , which is represented by first-order system.

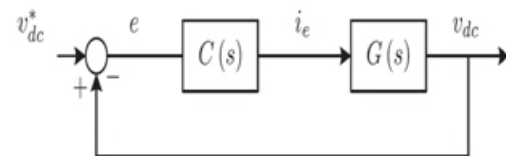


Figure 5: DC-voltage control block diagram.

IV.SIMULATION RESULTS:

A simulation model for the three-phase four-leg PWM converter with the parameters shown in Table I has been developed using MATLAB-Simulink. The objective is to verify the current harmonic compensation effectiveness of the proposed control scheme under different operating conditions. A six-pulse rectifier was used as a nonlinear load. The active filter starts to compensate at $t = t1$. At this time, the active power filter injects an output current iou to compensate current harmonic components, current unbalanced, and neutral current simultaneously.

During compensation, the system currents show sinusoidal waveform, with low total harmonic distortion (THD = 3.93%). At $t = t2$, a three-phase balanced load step change is generated from 0.6 to 1.0 p.u. The compensated system currents remain sinusoidal despite the change in the load current magnitude. Finally, at $t = t3$, a single-phase load step change is introduced in phase u from 1.0 to 1.3 p.u., which is equivalent to an 11% current imbalance.

As expected on the load side, a neutral current flows through the neutral conductor (iLn), but on the source side, no neutral current is observed (isn). Simulated results show that the proposed control scheme effectively eliminates unbalanced currents. Additionally, Fig. 8 shows that the dc-voltage remains stable throughout the whole active power filter operation.

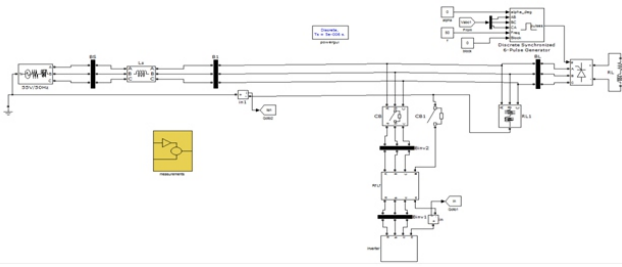


Fig 6: simulation design of proposed SAPF

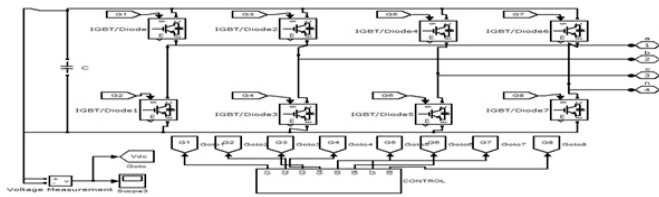


Fig 7: Four-leg converter circuit

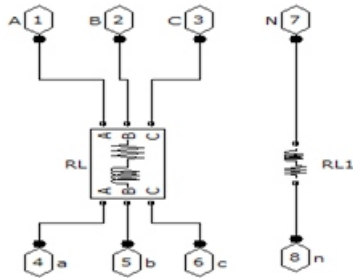


Fig 8: inductive filter

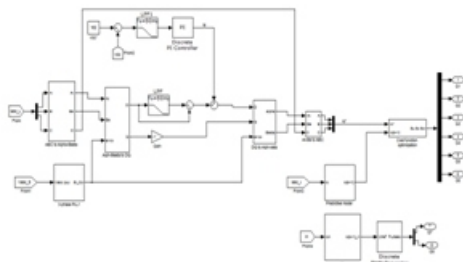


Fig 9: predictive digital current control circuit

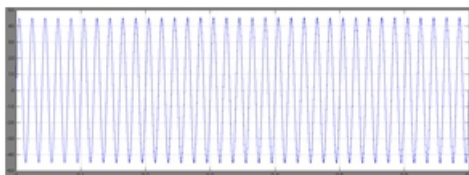


Fig 10: Phase to neutral source voltage

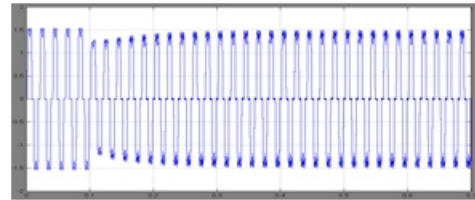


Fig 11: Load Current

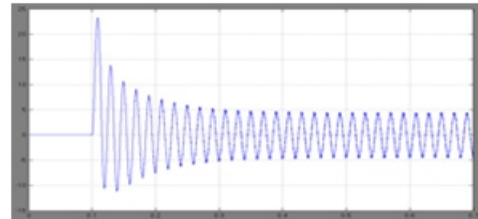


Fig 11: Active power filter output current.

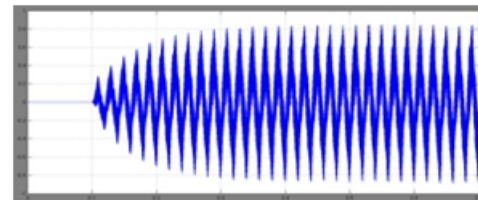


Fig 12: Load neutral current

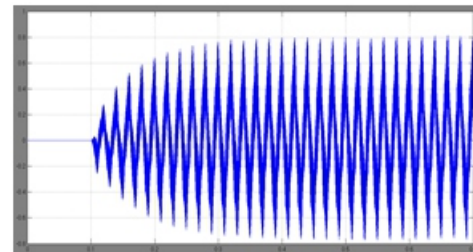


Fig 13: System neutral current

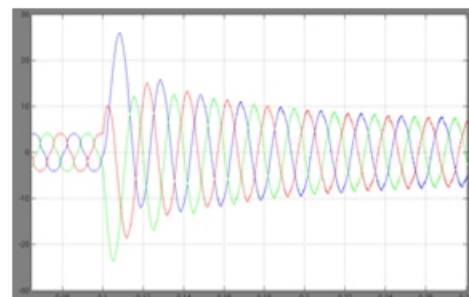


Fig 14: System currents

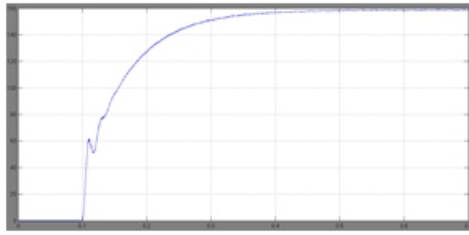


Fig 15: DC voltage converter

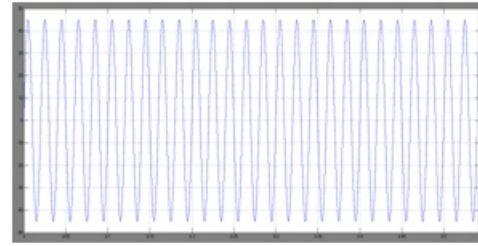


Fig 10: Phase to neutral source voltage

Implementation of SAPF with PV System:

This section presents an analysis and simulation of a PVinteractive Shunt Active Power Filter topology that achievessimultaneously harmonic current damping and reactive powercompensation. For the Shunt Active Filter reference currentcomputation, we used the Synchronous Reference FrameTheory (SRF). And for gating signal generation we apply thecarrier-based PWM modulation. Figure 16 shows the proposed system: a three phase source isconnected to a nonlinear load. A DC/DC converter can beused to adjust the value of the output voltage of PV energysource to the voltage value of the dc-side capacitor of theShunt Active Filter. The DC/DC converter is also responsible for tracking the maximum power point (MPPT) of the PV modules tofully utilize the PV power. Also, the inverter is always used toact as an active power filter to compensate the nonlinear loadharmonics and reactive power.

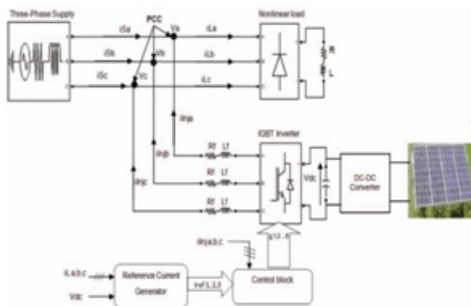


Fig 16: Configurations of photovoltaic interactive Shunt Active Filter system

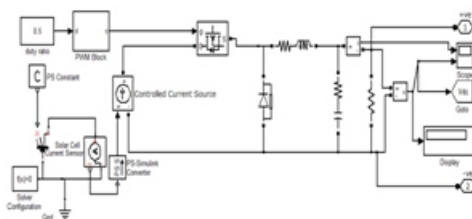


Fig 17: Simulink design of PV system

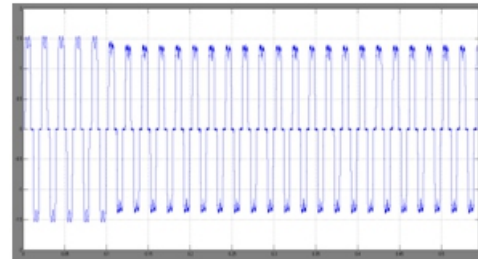


Fig 11: Load Current

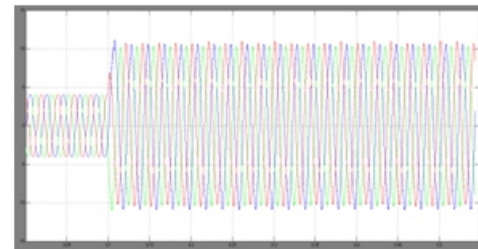


Fig 14: System currents

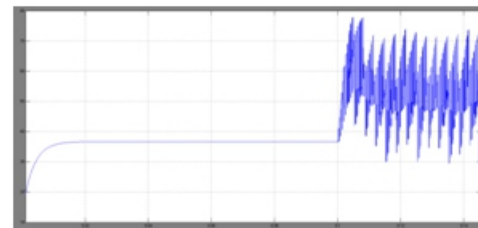


Fig 15: PV DC voltage

V.CONCLUSION:

Improved dynamic current harmonics and a reactive power compensation scheme for power distribution systems with generation from renewable sources has been proposed to improve the current quality of the distribution system. Advantages of the proposed scheme are related to its simplicity, modeling, and implementation. Simulated results have proved that the proposed predictive control algorithm is a good alternative to classical linear control methods.

The predictive current control algorithm is a stable and robust solution. Simulated results have shown the compensation effectiveness of the proposed active power filter with PV system.

REFERENCES:

- [1] J. Rocabert, A. Luna, F. Blaabjerg, and P. Rodriguez, "Control of power converters in AC microgrids," *IEEE Trans. Power Electron.*, vol. 27, no. 11, pp. 4734–4749, Nov. 2012.
- [2] M. Aredes, J. Hafner, and K. Heumann, "Three-phase four-wire shunt active filter control strategies," *IEEE Trans. Power Electron.*, vol. 12, no. 2, pp. 311–318, Mar. 1997.
- [3] S. Naidu and D. Fernandes, "Dynamic voltage restorer based on a fourleg voltage source converter," *Gener. Transm. Distrib.*, IET, vol. 3, no. 5, pp. 437–447, May 2009.
- [4] N. Prabhakar and M. Mishra, "Dynamic hysteresis current control to minimize switching for three-phase four-leg VSI topology to compensate nonlinear load," *IEEE Trans. Power Electron.*, vol. 25, no. 8, pp. 1935–1942, Aug. 2010.
- [5] V. Khadkikar, A. Chandra, and B. Singh, "Digital signal processor implementation and performance evaluation of split capacitor, four-leg and three h-bridge-based three-phase four-wire shunt active filters," *Power Electron.*, IET, vol. 4, no. 4, pp. 463–470, Apr. 2011.
- [6] F. Wang, J. Duarte, and M. Hendrix, "Grid-interfacing converter systems with enhanced voltage quality for microgrid application; concept and implementation," *IEEE Trans. Power Electron.*, vol. 26, no. 12, pp. 3501–3513, Dec. 2011.
- [7] X. Wei, "Study on digital pi control of current loop in active power filter," in *Proc. 2010 Int. Conf. Electr. Control Eng.*, Jun. 2010, pp. 4287–4290.
- [8] R. de Araujo Ribeiro, C. de Azevedo, and R. de Sousa, "A robust adaptive control strategy of active power filters for power-factor correction, harmonic compensation, and balancing of nonlinear loads," *IEEE Trans. Power Electron.*, vol. 27, no. 2, pp. 718–730, Feb. 2012.
- [9] J. Rodriguez, J. Pontt, C. Silva, P. Correa, P. Lezana, P. Cortes, and U. Ammann, "Predictive current control of a voltage source inverter," *IEEE Trans. Ind. Electron.*, vol. 54, no. 1, pp. 495–503, Feb. 2007.
- [10] P. Cortes, G. Ortiz, J. Yuz, J. Rodriguez, S. Vazquez, and L. Franquelo, "Model predictive control of an inverter with output LC filter for UPS applications," *IEEE Trans. Ind. Electron.*, vol. 56, no. 6, pp. 1875–1883, Jun. 2009.
- [11] R. Vargas, P. Cortes, U. Ammann, J. Rodriguez, and J. Pontt, "Predictive control of a three-phase neutral-point-clamped inverter," *IEEE Trans. Ind. Electron.*, vol. 54, no. 5, pp. 2697–2705, Oct. 2007.
- [12] P. Cortes, A. Wilson, S. Kouro, J. Rodriguez, and H. Abu-Rub, "Model predictive control of multilevel cascaded H-bridge inverters," *IEEE Trans. Ind. Electron.*, vol. 57, no. 8, pp. 2691–2699, Aug. 2010.